

(19)



Europäisches Patentamt

European Patent Office

Office européen des brevets



(11)

EP 0 859 453 B1

(12)

EUROPEAN PATENT SPECIFICATION

(45) Date of publication and mention
of the grant of the patent:
05.06.2002 Bulletin 2002/23

(51) Int Cl.7: **H02M 1/12**, H02M 7/06

(21) Application number: **98300780.8**

(22) Date of filing: **03.02.1998**

(54) **Power supply circuit for a control circuit**

Stromversorgung für Steuerschaltung

Circuit d'alimentation de puissance pour un circuit de contrôle

(84) Designated Contracting States:
**AT BE CH DE DK ES FI FR GB GR IE IT LI LU MC
NL PT SE**

(30) Priority: **14.02.1997 GB 9703088**

(43) Date of publication of application:
19.08.1998 Bulletin 1998/34

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EP-A- 0 654 886

- **PATENT ABSTRACTS OF JAPAN vol. 1997, no. 02, 28 February 1997 (1997-02-28) & JP 08 275547 A (TOSHIBA LIGHTING & TECHNOLOGY CORP), 18 October 1996 (1996-10-18)**
- **PATENT ABSTRACTS OF JAPAN vol. 1996, no. 08, 30 August 1996 (1996-08-30) & JP 08 103082 A (TOSHIBA LIGHTING & TECHNOLOGY CORP), 16 April 1996 (1996-04-16)**
- **PATENT ABSTRACTS OF JAPAN vol. 1997, no. 03, 31 March 1997 (1997-03-31) & JP 08 298778 A (TOSHIBA LIGHTING & TECHNOLOGY CORP), 12 November 1996 (1996-11-12)**

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Description

[0001] This invention relates generally to low voltage DC power supplies and more particularly to low voltage DC power supplies for control circuits.

[0002] In general, the "power factor" of an electrical load refers to the ratio of the active power provided to the load to the apparent power applied to the load. The power factor is closely tied to the phase relationship between the electrical current drawn by the load and the electrical voltage applied to the load from a source of electrical power. If the drawn current is sinusoidal and completely in-phase with an applied sinusoidal voltage, then a unity power factor (*i.e.*, a power factor of 1) is obtained.

[0003] High power factors are desirable for various reasons, including energy efficiency. The higher the power factor of a load, the lower the current demanded of the power supply utility for a given output power. Further, electronic loads with rectifier inputs and capacitive filtering frequently draw severely non-sinusoidal currents which results in poor power factor and can lead to distortion of the supply voltage. The higher the power factor, the lower the current that will be drawn from the supply for a given output power and the less the load will tend to distort the voltage waveform provided by the source of electrical power. To minimise supply currents and to avoid significant distortion of the voltage waveforms provided by power utilities, certain countries have promulgated regulations requiring electrical devices above a certain power rating to have a minimum power factor and limiting the harmonic content of the supply current.

[0004] In practice, electrical circuits often do not have unity power factors. In certain applications, such as motor control circuits that utilize a converter or inverter operating from a DC bus, the power factor can vary significantly from unity. Such circuits typically use a full wave bridge rectifier in combination with a relatively large DC bus capacitor to convert sinusoidal alternating input voltage into substantially constant direct voltage. In such arrangements, the rectifier output current should ideally follow the rectifier output voltage exactly. This is generally illustrated in Figure 1 which illustrates an ideal load in which the current drawn by the circuit (indicated by the dashed line) is substantially in-phase with the applied voltage (indicated by the solid line).

[0005] Power factor correction (PFC) circuits are often used to improve the power factor of a load by modifying the current drawn by the rectifier such that it approaches that shown in Figure 1. There are several commercially available PFC circuits. For example, Unitrode offers a family of high power-factor pre-regulator controllers under the model numbers UC1852, UC2852 and UC3852 and Linear Technology offers a power factor controller model number LT1248. These PFC devices are normally fabricated in analog integrated circuit chips and operate as analog circuits. In general, these devices

use pulse width modulated switching to improve the power factors of circuits, such as converters for switched reluctance motors, that utilize DC bus voltages derived from an alternating input.

[0006] Figure 2 illustrates the use of an exemplary analog PFC chip 14. The circuit receives applied sinusoidal alternating voltage at the inputs of a full wave rectifier 4 and produces a full wave rectified sinusoidal voltage. The full wave rectified sinusoidal voltage is applied to one terminal of a filtering inductor 8. Coupled to the other terminal of the inductor 8 is a switching device 10, such as a power MOSFET or an IGBT. The other terminal of the switching device 10 is coupled to the negative rail of the DC bus. A PFC chip 14 provides switching signals to switch the switching device 10 on and off. The PFC chip receives as inputs (a) a measure of the full-wave rectified sinusoidal voltage at the output of the bridge rectifier 4 (V_{SIN}), (b) a measure of the voltage across the DC bus (V_{RET}) and (c) a measure or estimate of the current flowing in inductor 8, commonly obtained using a resistive shunt to measure current in the switching device 10. A DC bus capacitor 6 is coupled across the positive and negative rails of the DC bus. A diode 12 is provided to prevent current from flowing back from the load when the switch 10 is closed. In operation, the PFC chip opens and closes switching device 10 so that the load across the full wave rectifier 4 varies from the inductor 8 (when switch 10 is closed) to the inductor and the DC bus capacitor 6 (when switch 10 is opened). By properly switching switch 10 the current in inductor 8 is made to follow a waveform corresponding to the voltage variations at the output of full wave rectifier 4. The power factor of the system is thus improved. The operation of PFC chips is generally understood and is not addressed herein in detail.

[0007] The magnitude of the alternating voltage applied to the input of the full wave rectifier 4 is typically fairly high (as much as 240 volts r.m.s.), as is the magnitude of the DC bus voltage that appears across capacitor 6 (as much as 400V d.c.). Most PFC control circuits, however, additionally require a DC supply voltage that is substantially less than the DC voltage that appears across the DC bus typically 10 to 20 volts. Accordingly, some mechanism must be provided for providing a relatively low DC supply voltage 14 to the PFC chip. Moreover, the low DC supply voltage provided to the PFC controller must be referenced to the negative rail of the DC link.

[0008] Many approaches have been used to supply the relatively low DC voltage to the PFC control circuit. Figure 3 illustrates one such approach. In Figure 3 the low DC supply voltage for the PFC controller is provided by a capacitor 20 that is charged through a high power bleed resistor 16. A zener diode 18 controls the voltage across capacitor 20. One significant disadvantage of DC voltage supplies that employ bleed resistors is that a large voltage is dropped across the bleed resistor, whilst the current flowing through the bleed resistor must be

at least equal to the current required by the PFC controller. This current produces considerable heat and represents a source of lost energy. This lost energy introduces inefficiencies into the system. A further disadvantage of DC voltage supplies using bleed resistors is that the bleed resistor must have characteristics capable of handling not only significant power dissipation but also the high voltage output of the full wave rectifier 4. Such resistors are often physically large, relatively expensive, and tend to increase the physical size and cost of systems using them.

[0009] Another common DC voltage supply for a PFC control circuit is illustrated in Figure 4. In this circuit a second inductor 26 is inductively coupled to the filter inductor 8. The second inductor 26 is coupled to a storage capacitor 24 via a diode 30. During operation, PFC controller 14 will switch switching device 10 on and off at a fairly high frequency. The high frequency voltage components appearing across the inductor 8 as a result of this switching induce a current flow and voltage in inductor 26 through transformer action. This current flows through diode 30 and charges capacitor 24 to the desired DC voltage. A bleed resistor 22 is provided to charge capacitor 24 when the circuit is first energized, before the transformer action is sufficient to charge capacitor 24. As before, a zener diode 18 serves to regulate the voltage applied to the control circuit.

[0010] While a bleed resistor is still required, it can be of a much higher resistance than that of Figure 3. The PFC control circuit will generally draw only a very small supply current until the capacitor 24 has charged to sufficient voltage to allow satisfactory operation of the PFC circuit. This allows resistor 22 to be of high resistance and hence the current flowing through it, and the power dissipated by it, will be relatively small. When the voltage across capacitor 24 has reached the required threshold, the PFC controller 14 will come into operation, drawing significant supply current. This current is initially supplied by capacitor 24 but is quickly supplied by the transformer action between inductors 8 and 26.

[0011] While the transformer-action DC voltage supply of Figure 4 reduces the need for a large bleed resistor, it does not eliminate the need for such a resistor. Accordingly, the DC voltage supply of Figure 4 suffers from the same disadvantages associated with the bleed resistor supply of Figure 3, although not to the same extent. The additional winding 26 significantly increases the size and cost of the inductor 8 with which it must be combined. Moreover, the transformer action circuit of Figure 4 is limited in that it is often insufficient to maintain an adequate voltage across capacitor 24. In these circumstances, it is necessary to reduce the value of resistance of the bleed resistor 22 to supplement the current from the inductor 26, bringing back the disadvantages already discussed.

[0012] In an effort to overcome the disadvantages associated with the circuits of Figures 3 and 4, approaches using more complex diode, capacitor and inductor ar-

rangements have been proposed. Figure 5 illustrates one such approach.

[0013] In Figure 5 a circuit is provided in which capacitors 34 and 46 are arranged with diodes 32 and 36 to form a charge pump circuit. The charge pump circuit charges capacitor 46 which provides a DC voltage to the PFC chip 14.

[0014] As with the circuit of Figure 4, the circuit of Figure 5 includes a small bleed resistor 44 that is used to charge the capacitor 46 when the circuit is first energized. Zener diode 40 again serves to regulate the supply voltage to the PFC circuit. Once the PFC chip 14 is operational, the charge on capacitor 46 is maintained through the switching action of the PFC chip as follows. At an initial point in time, switching device 10 will be closed and the voltage at node A will be approximately the value of the negative rail of the DC bus (e.g., 0 volts). At this point, the voltage at node B will also be approximately 0 volts. At a later point in time, the operation of the PFC chip will have necessitated opening of switch 10. This will cause the voltage at node A to rise to approximately the value of the positive rail of the DC bus (e.g., 380 volts). The voltage across capacitor 34 cannot instantaneously change, and a charging current will flow through it as the voltage at node A rises. This charging current will bias diode 36 ON, and current will flow through capacitor 34, through diode 36 into capacitor 46, charging capacitor 46 to the desired low DC voltage level. Eventually, node A will reach the DC bus voltage approximately (e.g., 380V), and the charging current flowing through capacitor 34 will cease. At this time, node B will be at approximately the same potential as the low voltage supply to the PFC chip and determined by zener diode 40. This might typically be 20V, so that capacitor 34 is charged to a voltage of e.g., 360V. In summary, at the time the switching device 10 is opened, capacitor 34 acts as a current source providing charge to the power supply capacitor 46.

[0015] At a later point in time, the PFC chip will close switching device 10 and the voltage at node A will again drop to approximately 0 volts. This switching event will also effectively place capacitor 34 in parallel with diode 32. This will discharge capacitor 34 through switching device 10 and diode 32. As the above indicates, in the circuit of Figure 5 capacitor 34 approximates to a current source where the current is that charging capacitor 46 immediately after switching device 10 is opened, and where the capacitor discharges through switching device 10 immediately after switching device 10 is closed.

[0016] The DC voltage supply of Figure 5 is limited in several respects. Initially it must be noted that all of the charge used to charge the power supply capacitor 46 is provided from capacitor 34. Accordingly, to prevent undesirable variations in the low voltage power supply, capacitor 34 must be sized sufficiently large so that power supply capacitor 46 is always adequately charged. This requirement of a sufficiently large capacitor 34 is disadvantageous in at least two respects. First, the capacitor

34 must be capable of withstanding high voltages. The larger the capacitor 34, the greater the cost and size of the capacitor and, hence, the larger the cost of the system. Second, as discussed above, while the charging current of capacitor 34 is used to charge the power supply capacitor 46 when the switching device is open, the charge across the capacitor 34 is discharged through switching device 10 when the switching device 10 is closed. Accordingly, switching device 10 must be sized to handle not only a portion of the current flowing through the full wave bridge 4, but must also dissipate all the energy stored in capacitor 34 at each instant of switch closure. This generally increases both the cost and the size of switching device 10. Further, the additional power dissipation in switching device 10 due to capacitor 34 results in a loss of power and increases the system inefficiencies. A further disadvantage of the power supply of Figure 5 is that the power supply capacitor 46 is charged only when the switching device 10 is switched off. A still further disadvantage of the power supply of Figure 5 is that, while it may be sufficient to drive the PFC controller 14, it typically cannot be used to drive other circuits, *e.g.*, a motor control circuit or a system control circuit. Such a multi-purpose power supply would require significantly more output current than the circuit of Figure 5. While one could theoretically increase the size of capacitors 34 and 46, such increases would necessitate a corresponding increase in the power handling capability of switching device 10, increase the cost of the system, and decrease the efficiency of the system.

[0017] As the foregoing demonstrates, known power supplies for PFC controllers generally result in the use of relatively expensive components or produce significant inefficiencies in the system. Moreover, such power supplies typically can power only a PFC controllers and cannot power other circuits. It is an object of the present invention to overcome these and other problems in the prior art.

[0018] The present invention is defined in the accompanying independent claim. Some preferred features are recited in the dependent claims.

[0019] In accordance with one form of the present invention, a power supply circuit for a control circuit is provided. The power supply circuit generates a low voltage that powers the control circuit from a switched load connected to a high voltage DC bus. The power supply circuit includes a power supply capacitor having a first terminal and a second terminal for storing a low voltage used in powering the control circuit. The power supply circuit further includes a charging capacitor having a first terminal and a second terminal. The charging capacitor charges the power supply capacitor when the power supply circuit is connected to the DC bus. The first terminal of the charging capacitor receives an input voltage from the high voltage DC bus. The power supply circuit further includes a first rectifier having an anode and a cathode. The anode of the first rectifier is connected to

the second terminal of the charging capacitor and the cathode of the first rectifier is connected to the first terminal of the power supply capacitor. The power supply circuit further includes an inductor having a first terminal and a second terminal. The first terminal is connected to the second terminal of the first capacitor and the anode of the first rectifier. The inductor charges the power supply capacitor by inductive action when the power supply circuit is disconnected from the DC bus. Thus, the power supply capacitor is charged both when the power supply circuit is connected to the DC bus and when it is not.

[0020] The power supply circuit further may include a second rectifier having an anode and a cathode. The anode of the second capacitor is connected to the second terminal of the power supply capacitor and the cathode of the second rectifier is connected to the second terminal of the inductor. The power supply circuit may further include a third rectifier having an anode and a cathode. The anode of the third rectifier is connected to the second terminal of the power supply capacitor and the anode of the second rectifier and the cathode of the third rectifier is connected to the cathode of the first rectifier and the first plate of the power supply capacitor.

[0021] In one embodiment of the present invention, the first and second rectifiers are standard diodes and the third rectifier is a zener diode. In another embodiment of the present invention, the first and third rectifiers are standard diodes and the second rectifier is a zener diode.

[0022] In accordance with another aspect of the present invention, a switched reluctance motor system is provided. The system includes a motor, a DC bus having a high output voltage, and a converter circuit having at least one switching device for controlling the application of power from the DC bus to the motor. The system further includes a switching device for connecting the DC bus to an alternating voltage source. An electronic controller is also provided for controlling the switching devices in the converter circuit. The system further includes a power factor correction circuit for increasing the power factor of the system. The power factor correction circuit controls the switching device for connecting the DC bus to the alternating voltage source. In this aspect of the present invention, the power factor correction circuit and the electronic controller are powered by a power supply circuit of the type described above.

[0023] Other aspects and advantages of the present invention will become apparent upon reading the following detailed description and upon reference to the drawings in which:

Figure 1 is a graph of the output current of an ideal rectifier circuit which is indicated by the dashed line and is shown substantially in-phase with the output voltage (indicated by the solid line);

Figure 2 is a schematic diagram of a circuit using an analog PFC chip;

Figure 3 is a schematic diagram of a prior art power supply circuit for a PFC chip;

Figure 4 is a schematic diagram of another prior art power supply circuit for a PFC chip;

Figure 5 is a schematic diagram of yet another prior art power supply for a PFC chip;

Figure 6 is a schematic diagram of a power supply circuit for a control circuit according to the present invention;

Figure 7A is a graph of the voltage at node X of the circuit shown in Figure 6 at various points in the operation of the circuit;

Figure 7B is a graph of the voltage across the capacitor 50 in the circuit shown in Figure 6 at various points in the operation of the circuit;

Figure 7C is a graph of the current flowing through the capacitor 50 in the circuit shown in Figure 6 at various points in the operation of the circuit;

Figure 7D is a graph of the current flowing through the inductor 52 in the circuit shown in Figure 6 at various points in the operation of the circuit;

Figure 7E is a graph of the current flow through the diode 56 at various points in the operation of the circuit; and

Figure 8 is a schematic diagram of a power supply circuit according to the present invention which supplies power to a PFC chip and an electronic controller for a switched reluctance motor.

[0024] Similar reference characters indicate similar parts throughout the several views of the drawings.

[0025] Turning now to Figure 6, a relatively low DC voltage power supply for circuits such as PFC circuits is illustrated. Although the following example addresses the use of the low voltage power supply in connection with a power supply for a PFC chip, the illustrated power supply can be used to generate a relatively low DC supply voltage from a switched load connected to a relatively high DC power supply. In the power supply of Figure 6, the current provided to charge the power supply capacitor 58 is provided from two sources. A small percentage of the current that is used to charge the power supply capacitor 58 is provided from a relatively small capacitor 50 when the switching device is opened. A significantly greater percentage of the current used to charge the power supply capacitor 58 is provided via resonant action between inductor 52 and capacitor 50 when the switching device is closed. Because the great percentage of the current used to charge the power supply capacitor is provided by resonant action, capacitor 50 may be relatively small.

[0026] Referring to Figure 6, the low voltage power supply comprises a power supply capacitor 58 across which is coupled a zener diode 60. Zener diode 60 serves to regulate the voltage across the capacitor 58 and, accordingly, serves to regulate the voltage level of the low voltage power supply. Although the desirable breakdown voltage of zener diode 60 will vary from ap-

plication to application, in the example of Figure 6, the breakdown voltage is assumed to be approximately 20 volts.

[0027] The power supply capacitor 58 is coupled to an inductor 52 via a diode 56. The inductor 52 is coupled to the negative rail of the DC bus 6 via a diode 54. The inductor 52 is also coupled to a relatively small capacitor 50.

[0028] In Figure 6, the diode 54 is illustrated as a standard diode. In alternative embodiments, standard diode 54 may be replaced with a zener diode where the breakdown voltage of the zener diode is selected to be the desired low DC supply voltage. In such embodiments, zener diode 60 may be eliminated or replaced with a standard diode.

[0029] In operation, the circuitry of Figure 6 provides current to the power supply capacitor 58 such that capacitor 58 remains charged to the desired low DC supply voltage. Moreover, the circuitry of Figure 6 ensures that the amount of charge provided to power supply capacitor 58 is sufficient for the power supply as a whole to meet the output current requirements.

[0030] Unlike known systems, the circuitry of Figure 6 provides current to charge power supply capacitor 58 both when the switching device 10 is opened and when the switching device 10 is closed. Moreover, unlike known systems, the majority of the current used to charge power supply capacitor 58 is provided when the switching device 10 is closed.

[0031] The operation of the circuitry of Figure 6 may be best understood through consideration of Figure 6 in conjunction with the voltage and current waveforms of Figures 7A-7E. Figures 7A-7E generally illustrate various currents and voltages in the circuitry of Figure 6 over time.

[0032] Referring to Figures 6 and 7A-7E, there is an initial point in time T_0 when switching device 10 is closed and the voltages represented in Figures 7A-7E are substantially constant. At that time, because switching device 10 is closed, the voltage across switching device 10 (V_{M}) will be substantially zero as illustrated in Figure 7A. The voltage at node X in Figure 6 will also be substantially zero at T_0 . For reasons discussed more fully below, the voltage across capacitor 50 at time T_0 will be approximately the negative of the voltage provided by the low voltage DC power supply. Accordingly, the voltage at node Y will be approximately equal to the voltage provided by the low voltage DC power supply. As Figures 7C and D illustrate, at time T_0 there is no current flowing from capacitor 50 (*i.e.*, I_C is 0 amps), there is no current flowing through inductor 52 (*i.e.*, I_L is 0 amps) and there is no current flowing into the power supply capacitor 58 (*i.e.*, I_D is 0 amps).

[0033] At a point in time T_1 it is assumed that the switching device 10 is opened by, for example, a switching command from PFC chip 14. When switching device 10 is opened, the substantially constant current flowing in inductor 8 is directed to capacitor 50, and consequent-

ly, the voltage at node X (with reference to the negative rail of the DC bus) rises until it reaches V_M . At this time, diode 12 becomes forward-biased and the current from inductor 8 flows into the DC bus capacitor 6 which, in the example of Figure 6, is charged to approximately 385 volts. This is illustrated in Figure 7A.

[0034] The charging current flowing through capacitor 50, as the voltage at node X rapidly rises from approximately 0 volts to approximately 385 volts, is forced to flow through diode 56 and, therefore, also into the network comprising capacitor 58 and zener diode 60. The capacitor 58 is thereby kept charged to the breakdown voltage of the zener diode 60, as desired. The voltage at node Y will correspondingly rise to a voltage of approximately 20 volts above the DC bus negative rail, while the voltage across the capacitor 50 rises in a linear fashion due to approximately constant current flowing into it from inductor 8. In this manner, the voltage across capacitor 50 rises from approximately -20 volts to approximately 365 volts. This is generally illustrated in Figure 7B where the voltage across capacitor 50 (V_C) is illustrated and in Figure 7E where the current I_D is shown.

[0035] At a time T_2 after switching device 10 is opened, the voltage across capacitor 50 will have risen to the level of approximately 365 volts and the voltage at node X will have correspondingly risen to approximately 385 volts. At this point, the current flowing into capacitor 50 (I_C) and the current flowing into the power supply capacitor 58 (I_D) will return to zero. In the circuitry of Figure 6, the relative sizing of capacitor 50 is such that the time interval between time T_1 and T_2 is relatively brief. For example, if it is assumed that at the time switching device 10 is opened the current flowing through switching device 10 was approximately 9.6 amps, the rate of change of the voltage across capacitor 50 will be approximately (9.6 A/ 179 pico-farads) or 53.6 kV/micro-second. Accordingly, it would take approximately (365V/(53.6 kV/micro-second)) or 6.8 nanoseconds for the voltage across capacitor 50 to reach 365 volts. Thus, the time interval between T_1 and T_2 is approximately 6.8 nanoseconds.

[0036] The voltage and current levels that exist in the circuit of Figure 6 will remain constant for a relatively long time interval during which switching device 10 remains open. At a later point in time T_3 switching device 10 will be closed again, e.g., in response to a command from PFC chip 14.

[0037] At the time T_3 when switching device 10 is closed, the voltage across the switching device 10 (V_M), and the voltage at node X, will begin to rapidly drop from its initial value of 385 volts towards a value of approximately zero volts. As discussed above, the voltage across a capacitor cannot instantaneously change. Accordingly, as the voltage at node X drops from a value of near 385 volts towards zero volts, the voltage at node Y will change from a voltage of approximately 20 volts to a voltage of approximately -365 volts. At this time,

because the voltage at node Y is less than the voltage on the negative rail of the DC bus, diode 54 will be biased on and a current I_L will begin to flow from the negative rail of the DC bus through diode 54 and into inductor 52 and returning to the negative rail of the DC bus through capacitor 50 and switching device 10. This is illustrated in Figure 7D. Note that, between T_3 and T_4 , the current in capacitor 50 is the negative of the inductor current I_L .

[0038] As the negative current I_C through capacitor 50 builds resonantly, the voltage at node Y will begin to rise from -365 volts towards a positive voltage. As the voltage at node Y rises, it will rapidly reach a point where the voltage at node Y reaches and exceeds zero volts. When the voltage at node Y rises to a level of approximately 20 volts (the voltage across power supply capacitor 58) diode 56 will be biased ON. In the example of Figures 6 and 7A-7E, this event occurs at a time T_4 . At this point in time, a current I_D will begin to flow through diode 56 into the power supply capacitor 58, charging the capacitor. This is illustrated in Figures 7D and 7E. The current I_D will continue to flow from inductor 52 to the power supply capacitor 58 until the current drops to near zero at a time T_5 .

[0039] Through use of the circuitry of Figure 6 it is possible to charge the power supply capacitor 58 with current provided primarily from the resonant action of capacitor 50 with inductor 52, as opposed to current solely from the charging of capacitor 50. This is possible because approximately the same amount of charge that is introduced into capacitor 50 when switching device 10 is opened is discharged from capacitor 50 into the power supply capacitor 58 when the switching device 10 is closed. Accordingly, by proper sizing of inductor 52, it is possible to maintain an adequate charge on power supply capacitor 58 with a relatively small capacitor 50. The use of a smaller capacitor 50 reduces the amount of current that switching device 10 must handle, potentially reducing the size and cost of switching device 10 and reducing the inefficiencies introduced when the capacitor discharges through the switching device.

[0040] The precise sizing of capacitor 50 and inductor 52 will vary by application according to, *inter alia*, the switching frequency of the switching device and the current drain that will exist on the power supply capacitor 58. In general, however, the following guidelines apply. In embodiments where it is desirable to minimize the size of capacitor 50, inductor 52 should be sized such that most of the current required to maintain an adequate charge on the power supply capacitor is obtained by resonant action when switching device 10 is closed.

[0041] The amount of charge provided over one cycle from the inductor 52 to the power supply capacitor 58 will be approximately $I^2/2 * L/V_{58}$, where I is the peak resonant current flowing through the inductor, L is the value of inductor 52 and V_{58} is the desired voltage across the power supply capacitor 58. In this example, V_{58} is 20 volts, so the charge provided during each

switching operation is approximately $I^2L/40$. In addition to providing adequate current to power supply capacitor 58, the inductor 52 must be sized such that the current flowing in the inductor returns to zero between switching events of the switching device. For example, if the switching frequency of the switching device is 100kHz (a period of 10 microseconds), the inductor should be selected to deflux completely in less than 10 microseconds. In this example, a suitable deflux period for inductor 52 would be 7 microseconds. The deflux period of the inductor 52 is approximately IL/V_{58} . Accordingly, for a deflux period of 7 microseconds (with a V_{58} of 20 volts) IL should be approximately 140 microsecond-volts.

[0042] Having selected a suitable deflux period for the inductor 52 an appropriate inductor size may be selected given the current drain on the power supply capacitor. Assuming that the average current drain on the power supply capacitor is 60mA and that the switching period is 10 microseconds, then the current from the inductor $I^2L/40$ must be 60mA * 10 microseconds. Assuming also a desired discharge period of 7 microseconds, it is known that IL must be approximately 140 microsecond-volts. Solving for I and L yields a peak resonant current I of 171 mA and an inductance for inductor 52 of 816 microhenrys.

[0043] Assuming a lossless resonant transfer of the energy stored in capacitor 50 to inductor 52 when switching device 10 is closed, the peak energy stored in the inductor must be equal to the energy stored in capacitor 50 at T_3 . Mathematically $CV^2=LI^2$ where C is the capacitance of capacitor 50, V is the peak voltage across capacitor 50, L is the inductance of inductor 52 and I is the peak resonant current through inductor 52. Because V is known (365V), L is known (816 microhenrys) and I is known (171 mA), C may be calculated at 179 pF.

[0044] Having determined the values of L and C it is now possible to determine the contributions of each towards the charging of power supply capacitor 58. As the above indicates, the inductor 52 provides current to charge the power supply capacitor 58 over a time interval of approximately 7 microseconds. Assuming that the current flowing through power switching device is 9.6 Amps when switching device 10 is opened, capacitor 50 will provide current to capacitor 58 for an interval of (365 volts * 179 picofarads)/9.6 amps or 0.0068 microseconds.

[0045] As the above indicates, in the circuit of Figure 6, the amount of time over which current flows through capacitor 50 to the power supply capacitor, equal to $T_2 - T_1$ (and in the example, approximately equal to 0.0068 microseconds) is significantly less than the amount of time current flows from inductor 52 to the power supply capacitor 58 equal to $T_5 - T_4$ (and in this example, approximately equal to 7 microseconds). Although the magnitude of current flowing into the capacitor 58 between T_1 and T_2 exceeds that flowing between times T_4 and T_5 , the fact that the second interval is much greater

means that the significant majority of the average current that maintains the desired voltage level across power supply capacitor 58 is provided by inductor 52 allowing for the use of a small and inexpensive capacitor 50. In addition, when the low DC voltage power supply of the present invention is used, a lower power switching device 10 may be used resulting in a lower cost system, because less additional current flows through the switching device and there are fewer losses in it. This results in a more efficient system.

[0046] The power supply circuit of Figure 6 is advantageous in that it provides a power supply that may be used to drive other control circuits in addition to PFC chip 14. For example, the power supply circuit of the present invention may be used in a switched reluctance motor system to power both PFC controller and an electronic controller used to control the motor. One such embodiment is illustrated in Figure 8. Figure 8 generally illustrates a switched reluctance motor system including a switched reluctance motor 90, a converter circuit 92 for controlling the application of power from the DC link to the motor 90 and an electronic controller 94 that controls the switching devices in the converter circuit 92. A PFC controller 96 is used to increase the power factor of the system. The electronic controller 94 may be of conventional construction as is taught in The Characteristics, Design and Applications of Switched Reluctance Motors and Drives, by Stephenson and Blake and presented at the PCIM '93 Conference and Exhibition at Nuremberg, Germany, June 21-24, 1993. Electronic controller 94 is supplied with a low DC voltage from a supply 98 which is of the type illustrated in Figure 6. As illustrated, the power supply terminals of the electronic controller 94 are coupled across the power supply capacitor 58.

[0047] The above description of several embodiments is made by way of example and not for purposes of limitation. In particular, the invention is applicable to switched reluctance machines having numbers of stator and rotor poles different from those illustrated above. The present invention is intended to be limited only by the scope of the following claims.

Claims

1. A power supply circuit comprising:

- a first capacitor (50) having a first terminal (X) and a second terminal (9), the first terminal of said first capacitor receiving an input voltage;
- a first rectifier (56) having an anode and a cathode, the anode of said first rectifier being connected to the second terminal (9) of the first capacitor (50);
- a serially connected combination of elements having a first end and a second end, the combination comprising an inductor (52) and a sec-

ond rectifier (54) which is connected to conduct from the second end to the first end, the first end being connected to the second terminal (9) of the first capacitor (50); and
 a second capacitor (58) having a first terminal and a second terminal, the first terminal of said second capacitor being connected to the cathode of the first rectifier (56) and the second terminal of said second capacitor being connected to the second end of the said combination of elements, wherein said second capacitor supplies an output voltage on application of the input voltage which is less than said input voltage.

2. The power supply circuit according to claim 1, further comprising a third rectifier (60) having an anode and a cathode, the anode of said third rectifier being connected to the second terminal of said second capacitor (58) and the cathode of said third rectifier being connected to the first terminal of said second capacitor (58).
3. The power supply circuit according to claim 2, wherein the first and second rectifiers (56, 54) are diodes.
4. The power supply circuit according to claim 3, wherein the third rectifier (60) is a zener diode.
5. The power supply circuit according to claim 2, wherein the first and third rectifiers are diodes.
6. The power supply circuit according to claim 5, wherein the second rectifier is a zener diode.
7. The power supply circuit according to claim 1, wherein the second rectifier is a zener diode.
8. A power circuit for an electrical load comprising a power supply circuit as claimed in any of claims 1 to 7, a dc bus arranged to derive its power from the input voltage at the first terminal (X) of the first capacitor (50) of the power supply circuit, a convertor (92) for controlling the transmission of power between the dc bus and the load, and switch means (10) operable to short circuit the input voltage and thereby regulate the input voltage to enable the power supply circuit.
9. The power circuit of claim 8 including a control circuit, wherein the power supply circuit is arranged to apply the said output voltage to the control circuit (14).
10. The power circuit of claim 9, the power having a power factor, wherein the control circuit (14) includes a power factor correction circuit arranged to

actuate the switch means (10) to vary the power factor of the power circuit.

11. The power circuit of claim 9 or 10 wherein the control circuit includes a controller for controlling the convertor.
12. A switched reluctance drive comprising a power circuit as claimed in claim 8, 9, 10 or 11 in which the electrical load includes the or each phase winding of a reluctance machine.

Patentansprüche

1. Stromversorgung, umfassend:

einen ersten Kondensator (50) der einen ersten Anschluß (X) und einen zweiten Anschluß (9) besitzt, wobei der erste Anschluß des ersten Kondensators eine Eingangsspannung aufnimmt;

einen ersten Gleichrichter (56) mit einer Anode und einer Kathode, wobei die Anode des ersten Gleichrichters mit dem zweiten Anschluß (9) des ersten Kondensators (50) verbunden ist; eine seriell verschaltete Kombination von Elementen, mit einem ersten Ende und einem zweiten Ende, wobei die Kombination eine Induktanz (52) und einen zweiten Gleichrichter (54) umfaßt, welcher derart verbunden ist, daß er von dem zweiten Ende zu dem ersten Ende leitet, wobei das erste Ende mit dem zweiten Anschluß (9) des ersten Kondensators (50) verbunden ist; und

einen zweiten Kondensator (58) mit einem ersten Anschluß und einem zweiten Anschluß, wobei der erste Anschluß des zweiten Kondensators mit der Kathode des ersten Gleichrichters (56) verbunden ist und der zweite Anschluß des zweiten Kondensators mit dem zweiten Ende der Kombination von Elementen verbunden ist, wobei der zweite Kondensator beim Anlegen der Eingangsspannung eine Ausgangsspannung zur Verfügung stellt, die kleiner ist, als die Eingangsspannung.

2. Stromversorgung nach Anspruch 1, weiterhin umfassend einen dritten Gleichrichter (60) mit einer Anode und einer Kathode, wobei die Anode des dritten Gleichrichters mit dem zweiten Anschluß des zweiten Kondensators (58) verbunden ist und die Kathode des dritten Gleichrichters mit dem ersten Anschluß des zweiten Kondensators (58) verbunden ist.
3. Stromversorgung nach Anspruch 2, wobei die ersten und zweiten Gleichrichter (56, 54) Dioden sind.

4. Stromversorgung nach Anspruch 3, wobei der dritte Gleichrichter (60) eine Zenerdiode ist.
5. Stromversorgung nach Anspruch 2, wobei die ersten und dritten Gleichrichter Dioden sind. 5
6. Stromversorgung nach Anspruch 5, wobei der zweite Gleichrichter eine Zenerdiode ist.
7. Stromversorgung nach Anspruch 1, wobei der zweite Gleichrichter eine Zenerdiode ist. 10
8. Starkstromleitung für eine elektrische Last, umfassend eine Stromversorgung nach einem der Ansprüche 1 bis 7, mit einem Gleichstrombus, der angeordnet ist, um seine Leistung aus der Eingangsspannung an dem ersten Anschluß (X) des ersten Kondensators (50) der Stromversorgung abzuleiten, einen Stromrichter (92), zur Steuerung der Leistungsübertragung zwischen dem Gleichstrombus und der Last und Schalteinrichtungen (10), einsetzbar für den Kurzschluß der Eingangsspannung und damit zur Regulierung der Eingangsspannung zum Einschalten der Stromversorgung. 15
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9. Starkstromleitung nach Anspruch 8, mit einem Steuerschaltkreis, wobei die Stromversorgung derart angeordnet ist, daß sie die Ausgangsspannung an den Steuerschaltkreis (14) anlegt. 25
10. Starkstromleitung nach Anspruch 9, wobei die Leistung einen Leistungsfaktor hat, wobei der Steuerschaltkreis (14) einen Leistungsfaktorkorrekturschaltkreis umfaßt, der derart angeordnet ist, um die Schalteinrichtungen (10) zu betätigen, um den Leistungsfaktor der Starkstromleitung zu variieren. 30
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11. Starkstromleitung nach Anspruch 9 oder 10, wobei der Steuerschaltkreis einen Controller zur Steuerung des Stromrichters umfaßt. 40
12. Geschalteter Reluktanzantrieb mit einer Starkstromleitung gemäß den Ansprüchen 8, 9, 10 oder 11, wobei die elektrische Last die oder jede Phasenwindung einer Reluktanzmaschine umfaßt. 45

Revendications

1. Circuit d'alimentation en puissance comprenant : 50
 - une première capacité (50) ayant une première borne (X) et une seconde borne (9), la première borne de ladite première capacité recevant une tension d'entrée; 55
 - un premier redresseur (56) ayant une anode et une cathode, l'anode dudit premier redresseur étant connectée à la seconde borne (9) de la première capacité (50);
 - une combinaison d'éléments, connectée en série, ayant une première et une seconde extrémité, la combinaison comprenant une enductance (52) et un second redresseur (54) qui est connecté de façon à conduire le courant depuis la seconde extrémité à la première, la première extrémité étant connectée à la seconde borne (9) de la première capacité (50); et
 - une seconde capacité (58) ayant une première borne et une seconde borne, la première borne de ladite seconde capacité étant connectée à la cathode du premier redresseur (56) et la seconde borne de ladite seconde capacité étant connectée à la seconde extrémité de ladite combinaison d'éléments, circuit dans lequel ladite seconde capacité fournit une tension de sortie lors de l'application de la tension d'entrée, qui est inférieure à ladite tension d'entrée.
2. Circuit d'alimentation en puissance selon la revendication 1, comprenant en outre un troisième redresseur (60) ayant une anode et une cathode, l'anode dudit troisième redresseur étant connectée à la seconde borne de ladite seconde capacité (58) et la cathode dudit troisième redresseur étant connectée à la première borne de ladite seconde capacité (58).
3. Circuit d'alimentation en puissance selon la revendication 2, dans lequel les premier et second redresseurs (56, 54) sont des diodes.
4. Circuit d'alimentation en puissance selon la revendication 3, dans lequel le troisième redresseur (60) est une diode Zener.
5. Circuit d'alimentation en puissance selon la revendication 2, dans lequel les premier et troisième redresseurs sont des diodes.
6. Circuit d'alimentation en puissance selon la revendication 5, dans lequel le second redresseur est une diode Zener.
7. Circuit d'alimentation en puissance selon la revendication 1, dans lequel le second redresseur est une diode Zener.
8. Circuit de puissance pour une charge électrique, comprenant un circuit d'alimentation en puissance selon une quelconque des revendications 1 à 7, un bus à courant continu disposé de façon à détourner sa puissance de la tension d'entrée à la première borne (X) de la première capacité (50) du circuit d'alimentation en puissance, un convertisseur (92) pour régler la transmission de puissance entre le bus à courant continu et la charge, et un moyen de

commutation (10) utilisable pour court-circuiter la tension d'entrée et régler ainsi la tension d'entrée afin d'activer le circuit d'alimentation en puissance.

9. Circuit de puissance de la revendication 8, comprenant un circuit de commande, dans lequel le circuit d'alimentation en puissance est disposé de façon à appliquer ladite tension de sortie au circuit de commande (14). 5
10. Circuit de puissance de la revendication 9, la puissance ayant un facteur de puissance, dans lequel le circuit de commande (14) comporte un circuit de correction de facteur de puissance disposé de façon à actionner le moyen de commutation (10) afin de faire varier le facteur de puissance du circuit de puissance. 10 15
11. Circuit de puissance de la revendication 9 ou 10, dans lequel le circuit de commande comporte un dispositif de commande pour commander le convertisseur. 20
12. Dispositif d'entraînement à reluctance commutée comprenant un circuit de puissance selon la revendication 8, 9 10 ou 11 dans lequel la charge électrique comporte le bobinage ou chaque bobinage de phase d'une machine à reluctance. 25

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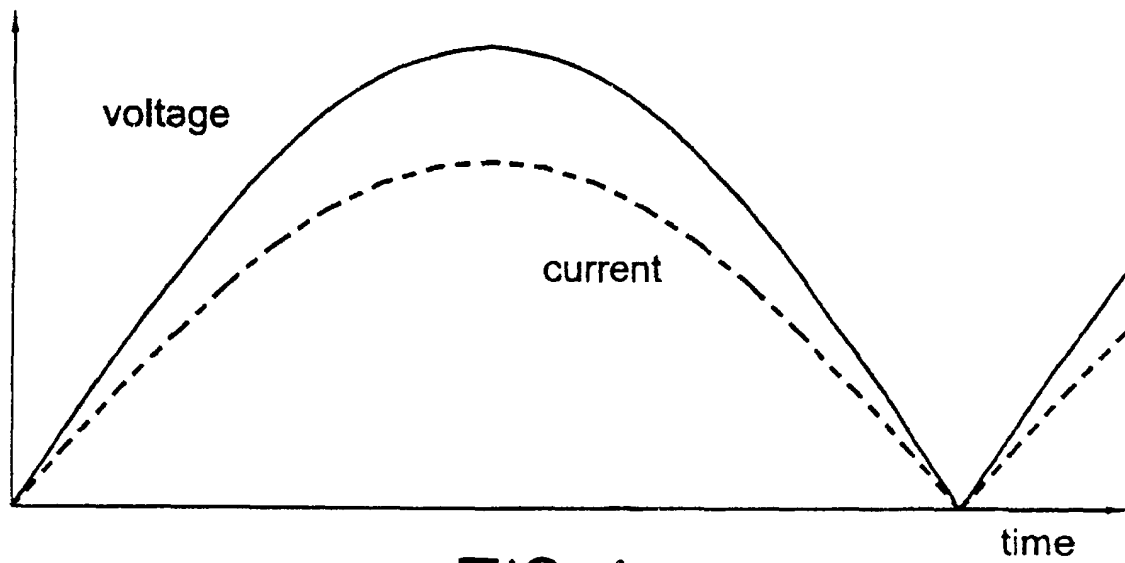


FIG. 1
PRIOR ART

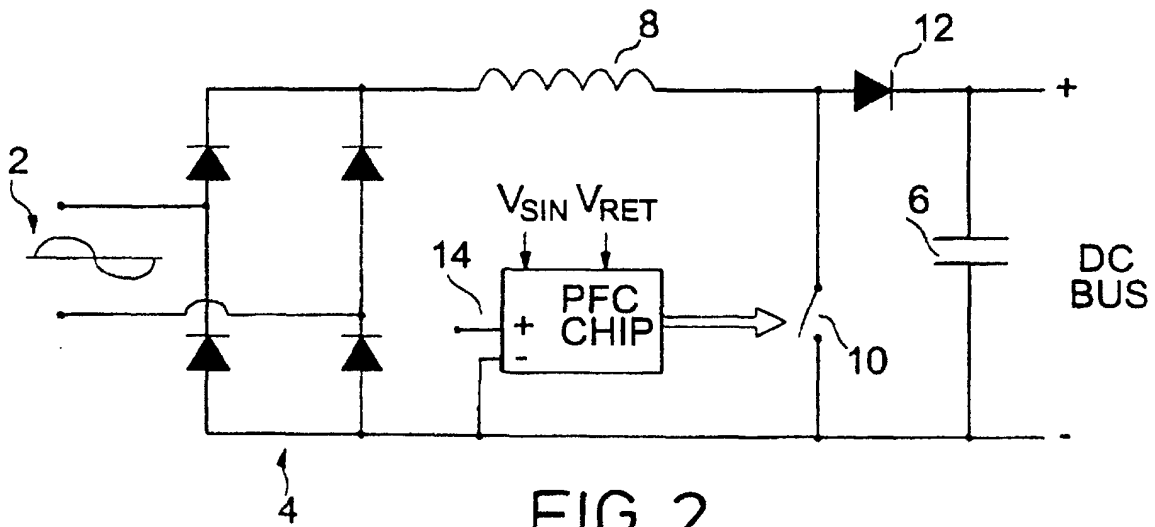


FIG. 2
PRIOR ART

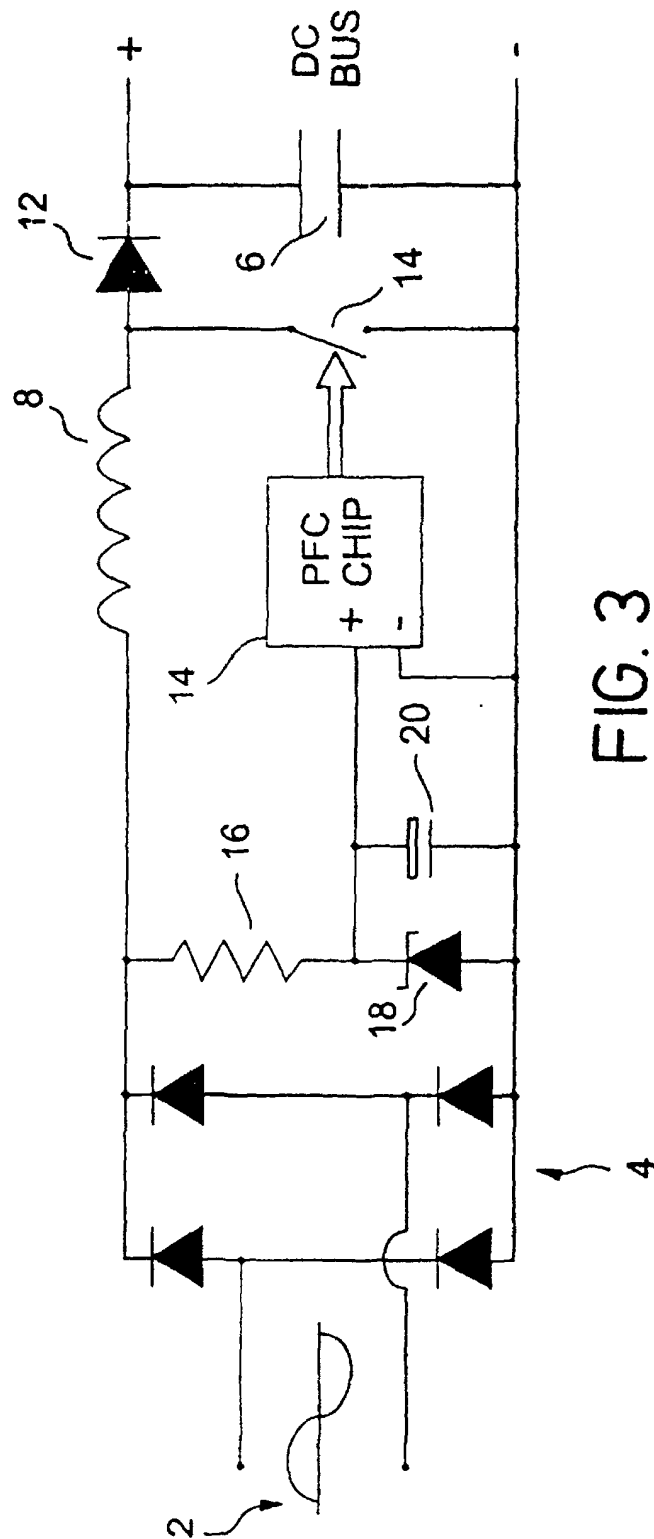
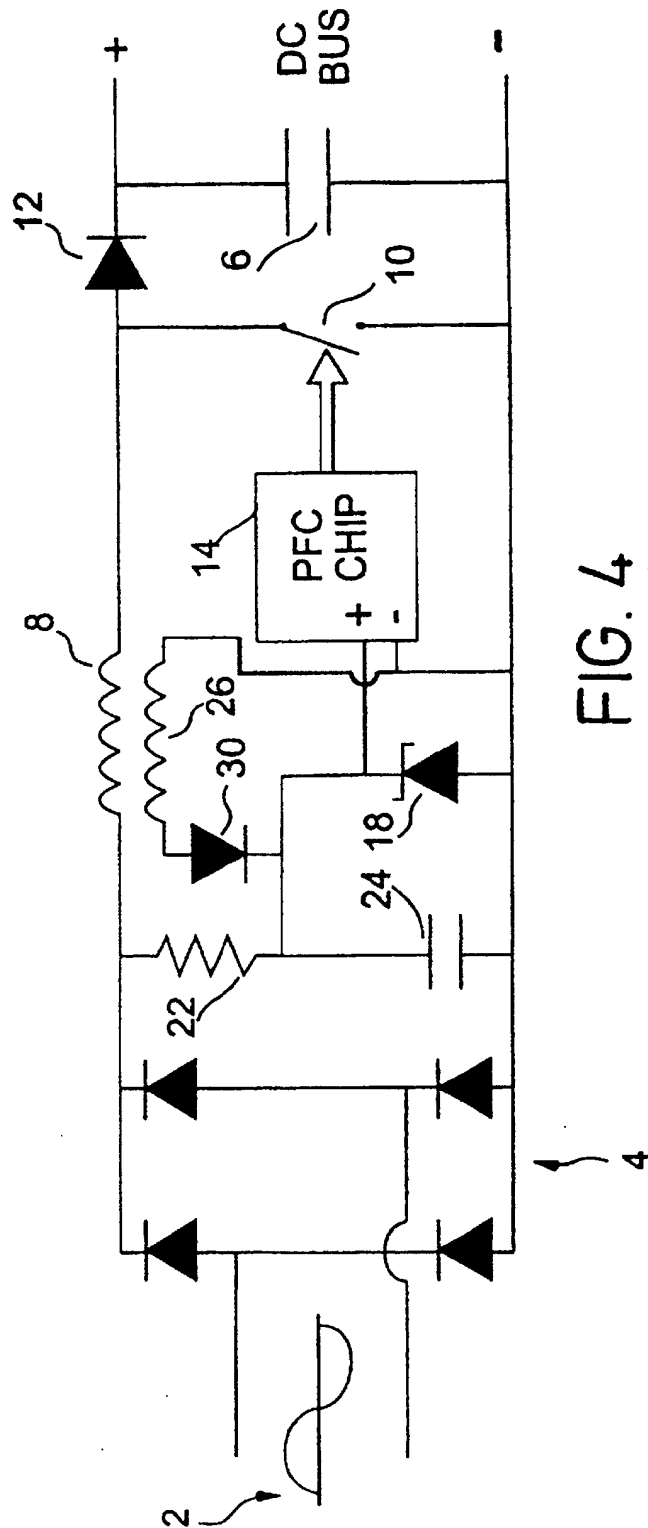


FIG. 3
PRIOR ART



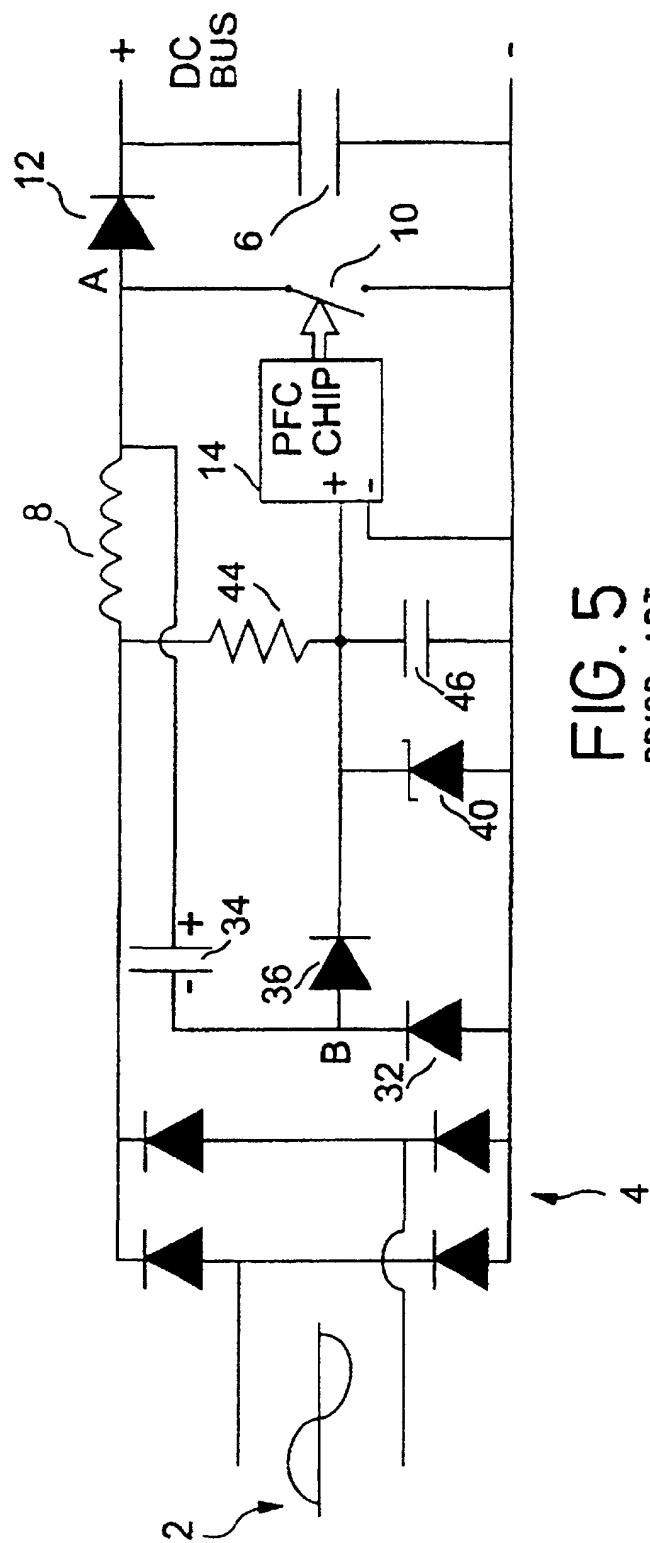
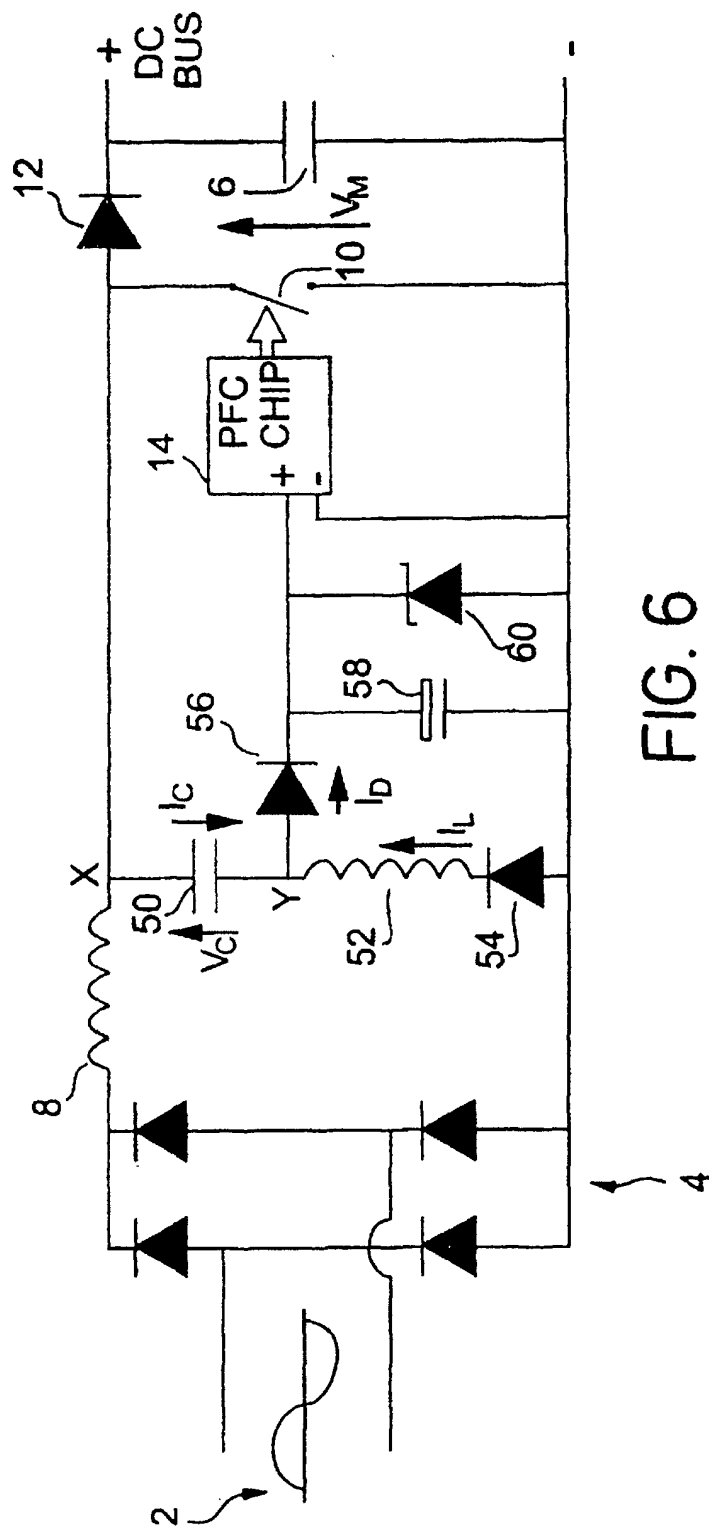


FIG. 5
PRIOR ART



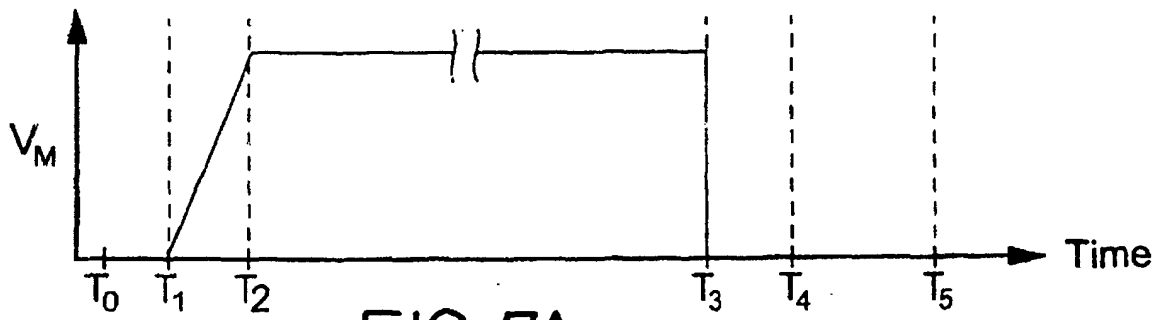


FIG. 7A

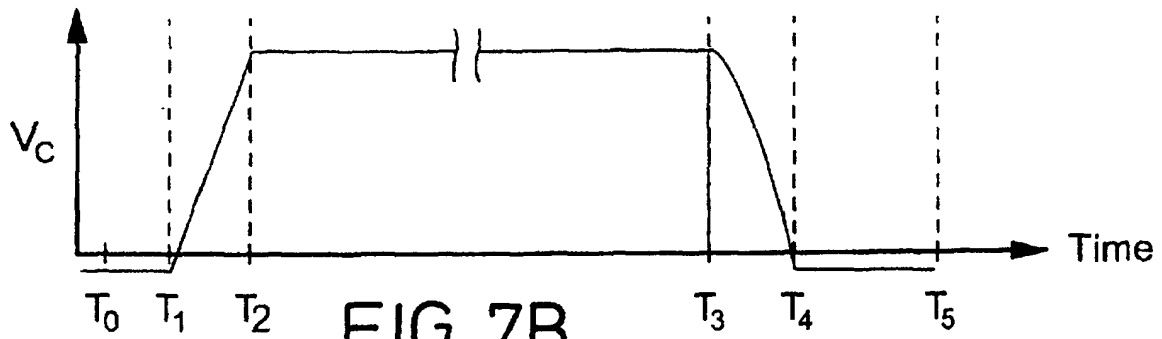


FIG. 7B

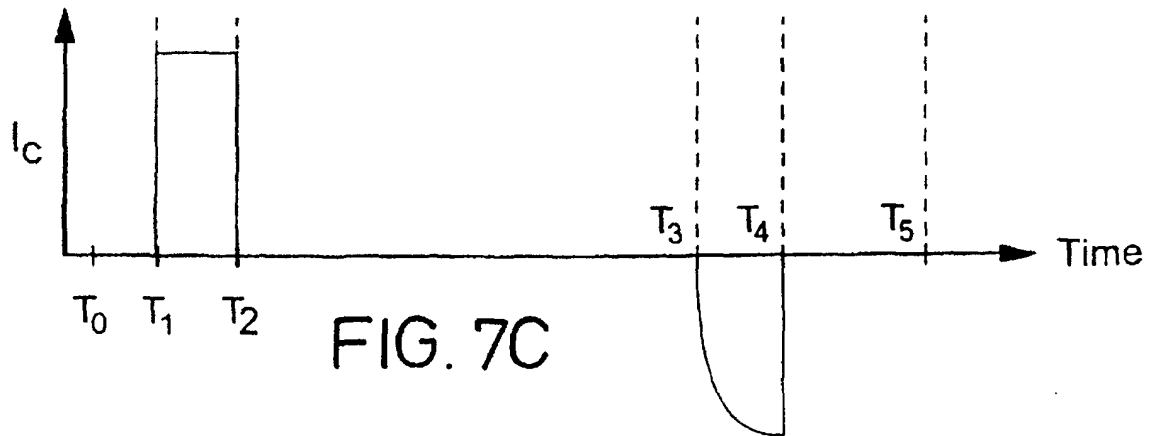
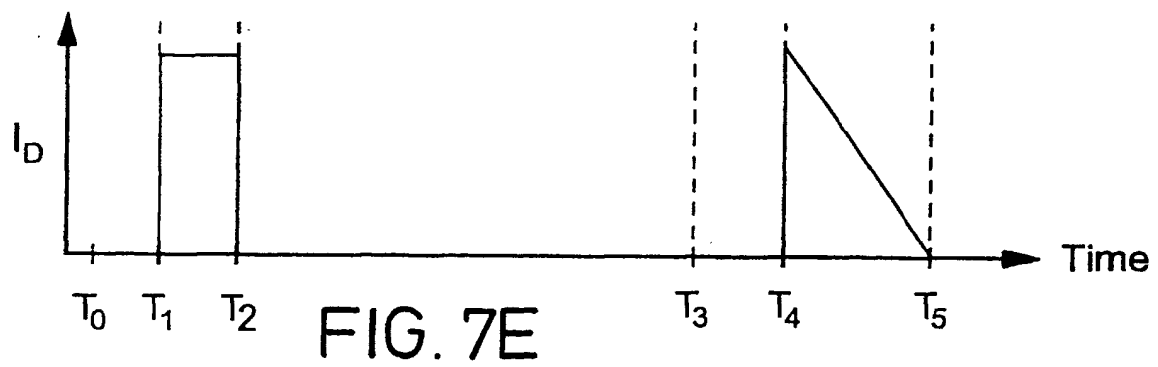
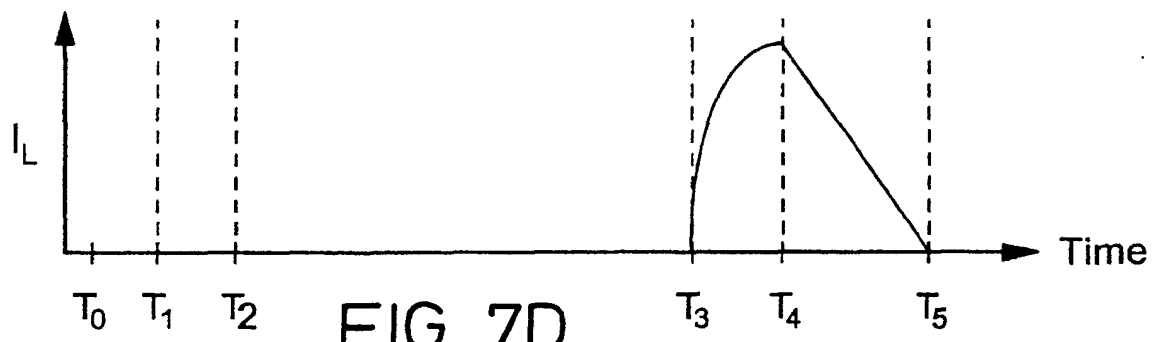


FIG. 7C



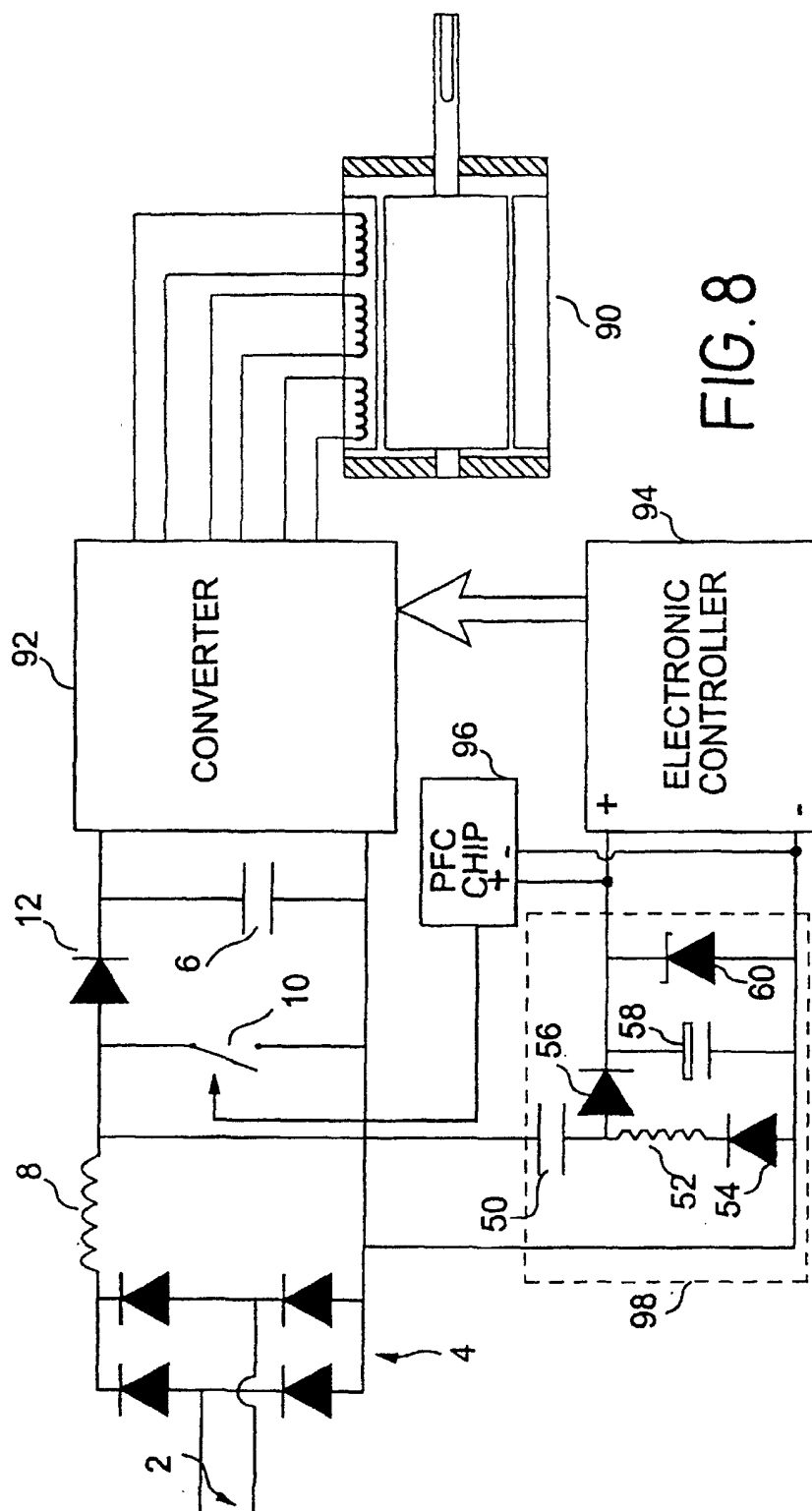


FIG. 8